Quad-active-bridge as cross-link for medium voltage modular inverters

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Suggested Citation
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Abstract—The Smart Transformer, a Solid-State transformer with control functionalities, is a promising smart grid technology. One of the main challenges of this system lies in making available a Medium-Voltage dc link, which can be tackled with modular solution. Thus, several isolated dc-dc converter can be used as a basic modules. In this paper, a Quad-Active-Bridge (QAB) dc-dc converter is used as modules for the entire dc-dc conversion stage of a ST. Besides the feature of high power density and soft-switching operation (also found in others converters), this converter offers an additional power path, named “MV cross-link” through the HF transformer in the Medium-Voltage (MV) side, increasing the power controllability among the MV cell without involving the LV side. To ensure soft-switching for all operation range of the QAB converter, the triangular current mode modulation strategy, previously study for the dual-active-bridge converter, is extended to the QAB converter in this work. In addition, it is considered to use in the MV side the H-Bridge cell and the multilevel neutral-point-clamped cell, to reduce the required voltage rating of the semiconductors. The theoretical analysis is performed for both converters. The theoretical analysis is verified by simulation and experimental results.

I. INTRODUCTION

In recent years, the smart grid technologies have received more and more attention, as a feasible solution to manage in an efficient way the growth in load and the high penetration of distributed generation (DG). One of these technologies is the Smart Transformer, which is a Solid-State Transformer [1] - [2] with control and communication functionalities [3]. This power electronics based system uses a high frequency (HF) transformer, reducing volume and space, and it can also provide ancillary services to the grid, such as: power factor correction, active filtering, VAR compensator, electronics protection and disturbance rejection [1] - [2].

The three-stage ST is usually composed by a Medium-Voltage (MV) ac-dc stage, a HF isolated dc-dc stage and a Low-Voltage (LV) dc-ac stage. The main challenge of this architecture is the dc-dc conversion stage, since it has strict requirements, such as: high rated power, high current capability in LV side, high voltage capability in HV side, high frequency isolation and high efficiency. To meet all requirements, two solutions have been widely investigated: the first one is to use standard converter with high voltage rating devices [4] - [6], while the second one is based on the modular concept, in which several modules are used to share the total voltage and power among them [7] - [13]. Although the modular solution presents high number components, it has several advantages compared to the fist solution, such as: low \( \frac{dv}{dt} \) (low EMI emission), possibility to use standard low voltage rating devices and also modularity, which allows to implement redundant strategy to increase the fault tolerance and reliability.

Several converters have been investigated to be used as module of the main core of the ST, but the Dual-Active-Bridge (DAB) and the Series-Resonant converter (SR) have received more attention, due its advantages of soft-switching, high efficiency and power density [8] - [13]. The Series-Resonant dc-
The Quad-Active-Bridge (QAB) dc-dc converter presents a well regulated output voltage for large range of load (when operating in discontinuous-conduction-mode), avoiding the requirement of control loops. For that reason, it is also called dc-transformer [11] - [13]. On the other hand, when controllability of the output voltage or power is required, the DAB converter is more advantageous, since it works with active control of the transferred power [8] - [10]. In addition, this converter can also control the power flow among the MV modules of the ST, however the LV bridge and the LVDC link are involved in the power conversion path, compromising the overall efficiency.

To reduce the number of power conversion during the power exchange of the MV modules, a converter that provides a direct power path among the MV modules can be used instead the DAB converter. The Quad-Active-Bridge (QAB) dc-dc converter, previously reported in [14] - [16], has all the described characteristics. This converter is composed by four actives bridges connected to the same four winding HF transformer, as depicted in Fig. 2 (a). For ST application, one bridge of the QAB converter should be connected to the LV side and the others three bridges should be connected to the MV side, in order to share the Medium-Voltage among them. In this configuration, the QAB dc-dc converter has the same advantages of the DAB, however with an additional feature of power transfer capability among the MV cells in a high efficiency way. As can be seen in Fig. 2, the QAB has a magnetic link that allow directly exchange of power among the MV cells without including the LV cell. In others words, the QAB offers an additional power path to the MV cells, named “cross-link”, which can increase the redundancy scheme and, consequently, the reliability of the system.

Similarly to the DAB converter, the QAB converter can also work with phase-shift modulation, where the power changed among two bridges is controlled by the shifted angle of one bridge in respect to the other. However, this modulation strategy might have some limitation on the soft-switching operation, when the input or output voltage varies. To overcome this problem, duty-cycle variation can be used to ensure soft-switching operation of the converter, as reported in [17].

In this context, this paper investigate the application of the QAB converter using the triangular current modulation strategy to a Smart Transformer, focusing only on the power converter performance. Fig. 1 shows the the block diagram of a ST employing the QAB converter as dc-dc solution and a Cascaded H-Bridge (CHB) for the MV ac-dc conversion stage. In this work, a power unit (highlighted in Fig. 1) can be defined as a replaceable part of the system. For this architecture, an unit is composed by an entire QAB converter and some modules of the CHB converter, but only those associated to the QAB converter of the unit, as can be seen in Fig. 1. The power cell is the smallest power block of the unit and it is also highlighted in Fig. 1. In architecture, it is chosen to use three units per phase, to have a good trade-off between number of components and effort among the same.
Table I shows the specification of a typical ST for distribution system application and also the specification of a single QAB converter of the ST, considering the configuration shown in Fig. 1. As it can be observed, the voltage of the MV bridges of the QAB converter is still high (1.13 kV). Using a standard H-bridge cell in the MV side, 1.7 kV IGBT are required. However, multilevel cell can also be employed in the MV side, in order to reduce the voltage of the semiconductors and to enable to use of 1.2 kV, which presents lower forward drop voltage and lower conduction losses. In this work, the NPC cell is also considered to be used in the MV cell of the QAB converter. Fig. 3 (a) and (b) shows the complete topology of the QAB dc-dc converter, employing NPC cell and HB cell in the medium voltage, respectively. Both cells are considered for study in this paper.

The main contribution of this paper in the field of QAB, is to evaluate the operation of the QAB converter using the triangular current modulation strategy for smart transformer application, where all the main equations for the design are derived. As an additional contribution, the operation of the QAB converter using a NPC cell is also investigate in this paper. The theoretical analysis is carried out considering the balancing condition (all MV bridges processing the same amount of power) and also unbalancing condition (all MV bridges processing the different amount of power) of the QAB converter. The operation principle of the QAB converter using the triangular current modulation strategy is presented in section II for balance condition, where the modulation strategy is described and the equations for the power transferred and current effort are described. The unbalance condition is discussed in section III. Finally, the simulation and experimental results are presented and discussed in section IV and the conclusion is presented in section V.

### II. OPERATION PRINCIPLE

The topology of the QAB is shown in Fig. 3 (a) and (b), considering different cells on the MV side. Regardless the cell, an equivalent circuit based on Y-model can be used to analyze the converter. In this equivalent circuit, the bridges are replaced by rectangular voltage source \( v_a, v_b, v_c \) and \( v_d \) (see Fig. 2) and the voltage of the central point \( v_z \) is given by (1). The current slope of each bridge can be defined by (2), where \( k \in \{ a, b, c, d \} \). As defined in Fig. 2, \( v_a \) is the ac voltage synthesized by the LV bridge, while the voltage \( v_b, v_c \) and \( v_d \) are the voltage of the MV cells. The power processed by the bridges named \( a, b, c \) and \( d \) are \( P_1, P_2, P_3 \) and \( P_4 \), respectively, and \( P_1 = P_2 + P_3 + P_4 \). As the HB converter is able to synthesize twice the total dc voltage (+\( V_{MV} \), 0 and -\( V_{MV} \)), while the NPC converter can synthesize only the total dc voltage (+\( V_{MV}/2 \), 0 and -\( V_{MV}/2 \)), the modulation analysis is carried out considering the HB converter. In this analysis, it is also considered that the all inductors have the same inductance value \( L_1 = L_2 = L_3 = L_4 = L \) and also that the power is transferred from the MV side to the LV side.

\[
sv = \frac{va + vb + vc + vd}{4}
\]

\[
\frac{di_{Lb}}{dt} = \frac{(vk - vs)}{L}
\]

### A. Triangular Current Mode Modulation Strategy

To modulate the converter, the Triangular Current Modulation Strategy (TCMS) presents an attractive solution [18]. By properly selecting the transformer turns ratio, the MV side switches can be operated in ZCS mode in both power directions while actively controlling the transferred power by adjusting the LV side duty cycle [17]. This strategy has been extensively investigated for the DAB converter [17] - [20], and in this paper, it is extended to the QAB converter.

Initially, it is considered that the QAB operates balanced, i.e. each MV bridge processes the same amount of power \( P_2 = P_3 = P_4 \). In this case, low voltage bridge operates with duty-cycle \( d_1 \) and all the three MV bridges operate with the same duty-cycle \( d_2 \).

The basic principle of this modulation strategy is to impose a triangular current on the inductors, as shown in Fig. 3 (d) and (e). To do that, the voltages \( vs \) and \( v_a \) should have the waveforms shown in Using this modulation strategy, the voltage \( v_z \) is given by (3) for this condition. The current \( i_{Lb} \), the voltages \( v_a, v_b \) and \( v_c \) are shown in Fig. 3 (d), for positive power flow, and (e) for negative power flow. As it can be observed, the current through the inductor starts from zero and reaches its maximum value \( \Delta i_{Lb} \) during the period of time between 0 and \( T_s \), where \( T_s \) is the switching period. The current variation during this period is described by (4). As the current starts from zero, the switches \( S_2 \) and \( S_3 \) of the LV side and also the switches \( S_5 \) and \( S_6 \) of the MV side turns-on at Zero-Current-Switching (ZCS). In this moment (\( t = D_1T_s \)), the Zero-Voltage-Switching will occur, but only if energy stored in the transformer inductance is enough to completely discharge the total equivalent output capacitance of the switch, as seen by the circuit, before it is switched on. Energy stored in the inductor depends on squared value of the peak current \( \Delta i_{Lb} \) at the moment transition occurs, while the total equivalent output capacitance of the switch includes switches built-in output capacitance, additional snubber and parasitic capacitances. Thus, the capacitors snubber should be designed to achieve the ZVS commutation.
\[ v_x = \begin{cases} 
\frac{nV_L + 3V_H}{4}, & 0 < t < d_2T_s \\
\frac{nV_L}{4}, & d_2T_s < t < d_1T_s \\
0, & d_1T_s < t < T_s/2 
\end{cases} \]

\[ \Delta i_{lb(0<t<d_2T_s)} = \frac{D_2(V_H - nV_L)}{4Lf_s} \]  

Likewise, during the period between \( D_1T_s \) and \( D_2T_s \), the current decrease from \( \Delta i_{lb} \) until reaches zero again. This variation is described by (5). In the instant \( D_2T_s \), the current is zero and the switch \( S_1 \) turned-off (at ZCS) and the MV bridge imposes \( v_a = 0 \). It is important to note that the period in zero state should be long enough to evacuate all charge accumulated at the IGBT during the conduction state. Thus, this commutation can be critical for rated load operation, where the stored charger is high and the zero time period is small [17]. To achieve ZCS operation regardless the load and input or output voltages levels, the condition (4)=(5) must be satisfied. As a result, the relation between the duty-cycle \( D_1 \) and \( D_2 \) is found and presented in (6).

\[ \Delta i_{lb(D_2T_s<t<T_s/2)} = \frac{nV_L(D_1 - D_2)}{4Lf_s} \]  

\[ D_2 = \frac{V_L \cdot n}{V_H} D_1 \]  

B. Power Transferred

The transferred power can be calculated on the dc side of the bridges by: \( P_{\text{avg}} = I_b V_k \), where \( k \) denotes the cell. The average current in the cell \( b \) \( (I_b) \) is calculated in (7). Thus, the power processed by the cell \( b \) (MV cell) and \( a \) (LV cell) are shown in (8).

\[ I_b = \frac{2}{T_s} \int_0^{D_2T_s} i_b (d) \, dt = \frac{D_2^2(V_H - nV_L)}{4Lf_s} \]  

\[ P_2 = \frac{D_1^2(V_Ln)(V_H - V_Ln)}{4Lf_s} \]  

\[ P_1 = \frac{3D_1^2(V_Ln)(V_H - V_Ln)}{4Lf_s} \]  

C. Current Efforts

From Fig. 3 (d), it is possible to calculate the current effort on the primary (LV side) and secondary (LV side) of the transformer. The rms current on the primary and secondary sides in function of the duty-duty \( D_1 \) is shown in (9) and (10).

\[ i_{\text{sec.rms}} = \frac{nV_L(V_H - nV_L)}{12Lf_s V_H} \sqrt{6d_1^3} \]  

\[ i_{\text{prim.rms}} = \frac{n^2V_L(V_H - nV_L)}{4Lf_s V_H} \sqrt{6d_1^3} \]  

The current waveform in each switch of the QAB converter is depicted in Fig. 4. Fig. (4) shows the current for the LV side bridge, while the Figs. (4) (b) and (c) shows the current for the MV side bridge, when it is implemented with HB and NPC, respectively.

As can be seen, the LV side switches commutate at ZCS during the turn-on and turn-off, as well the switches of the MV cell. For the switch \( S_2 \) of the MV cell and LV cell (see Fig. 4), the commutation are complete free of losses, since the current remains in zero for a while before the voltage starts to increase.

The current efforts in the LV bridge can be calculated from Fig. 4 (a) and efforts (rms and mean) for each semiconductors.
of the MV cell are presented from equation (11) to (12).

\[ i_{s1(rms)} = \frac{nV_L (V_H - nV_L)}{12LsV_H} \sqrt{3d_1^3} \]  \hspace{1cm} (11)

\[ i_{s1(avg)} = \frac{d_1^2 (nV_L)^2 (V_H - nV_L)}{8LsV_H} \]  \hspace{1cm} (12)

Similarly, the current efforts for the MV side, when the NPC cell is amployd, is obtained from Fig. 4 (c) and the efforts (rms and mean) for each semiconductors of this cell are presented from equation (13) to (18).

\[ i_{s1(rms)} = \frac{nV_L (V_H - nV_L)}{12LsV_H} \sqrt{3d_1^2 nV_L} \]  \hspace{1cm} (13)

\[ i_{s1(avg)} = \frac{d_1^2 (nV_L)^2 (V_H - nV_L)}{8LsV_H^2} \]  \hspace{1cm} (14)

\[ i_{s2(rms)} = \frac{nV_L (V_H - nV_L)}{12LsV_H} \sqrt{3d_1^3} \]  \hspace{1cm} (15)

\[ i_{s2(avg)} = \frac{d_1^2 (nV_L) (V_H - nV_L)}{8LsV_H} \]  \hspace{1cm} (16)

\[ i_{s1(rms)} = \frac{nV_L (V_H - nV_L)}{12LsV_H} \sqrt{3d_1^3} (V_H - nV_L) \]  \hspace{1cm} (17)

\[ i_{s1(avg)} = \frac{d_1^2 (nV_L) (V_H - nV_L)}{8LsV_H^2} \]  \hspace{1cm} (18)

For the MV side using the HB cell, the current efforts on the semiconductors are very similar to the NPC case. As can be observed in Fig. 4 (b) and (c), the waveform for the current \( i_{s1(HB)} \) of the HB cell is similar to the current \( i_{s1(NPC)} \) of the NPC cell. Thus, the current effort is defined by the same equation and already presented in (13) and (14). For the switch \( S_2 \) of the HB \( \left( i_{s2(HB)} \right) \), part of the current flows through the channel (positive part) and the other part flows through the diode (negative part). Thus, the effort can be calculate separately in this two element of the devices. The current the flows through the channel of the IGBT is similar to the current \( i_{s2(NPC)} \), then it can be calculated using also equations (15) and (16). Likewise, the current flowing through the intrinsic diode of the device \( S_2 \) (of the HB cell) is similar to current \( i_{s2(NPC)} \) and it can be calculated by (17) and (18). It is important to note that the equation to calculate the effort on the NPC cell and HB cell are very similar, but the parameters (mainly \( n, L \)) are different for the same output power. The current peak in the NPC cell is twice the current peak on the HB cell.

From these equation, the rms current on the primary side and secondary side in function of the output power are plotted in Fig. 5 (a), while the current efforts on the semiconductors are depicted in Fig. 5 (b).

III. UNBALANCE CONDITION

For unbalance condition \( (P_2 \neq P_3 \neq P_4) \), the duty cycle of the MV bridges are not equal anymore. The duty-cycle of each MV cell will depend on the power processed by them. For this analysis, it is considered that only the power of the cell \( b \) is different, i.e. \( P_2 \neq P_3 = P_4 \). Considering this condition, the voltages \( v_a, v_b \) and \( v_x \), as well as the current \( i_b \) and \( i_c \) are depicted in Fig. 6. As it can be observed, the current starts from a value different of zero, increase until reaches the maximum value, and then the current starts to decrease again until to reaches the same negative initial value. During the commutation, the current is not zero anymore, hence the ZCS feature is lost. Nevertheless, the current value during the commutation is very low, which indicates a very low switching losses. Actually, the switching losses will be proportional to the unbalanced load.

As the cell \( b \) is processing different amount of power compared to the cells \( c \) and \( d \), then its duty-cycle is also slightly different. The duty cycle of the cell \( b \) is \( D_{2b} \), while the duty cycle of the cells \( c \) and \( d \) is defined as \( D_{2c} \) and \( D_{2d} \). The slight difference of the duty-cycle cell \( b \) regarding the duty-cycle of cell \( c \) and \( d \) is defined as \( \Delta D_{2b} = D_{2b} - D_{2c} \).

As can be observed in Fig. 6, in the instant \( t = D_{2b}T_s \) the voltage \( v_b \) goes to zero, but the voltage \( v_c \) and \( v_d \) remains equal to \( V_H \) until the instant \( t = D_{2c}T_s \). Thus, the voltage \( v_x \) will have one more level, as can be seen in this figure. This additional level makes the current \( i_{b} \) decreases and the current \( i_c \) increases. Thus, the currents \( i_b \) and \( i_c \) has different behavior during this period of time between \( D_{2b}T_s \) and \( D_{2c}T_s \) (or called \( \Delta D_{2c} \)). Afterwards, both current decreases with the same slope, but they achieve different values, because they start from different points. As a conclusion, the variable \( \Delta D_{2b} \) has direct impact on the dc value of the currents, and consequently the additional power delivered by the MV cell. For that reason, this new variable can be used to control the power exchange among the MV cells. The Figs. 7 (a) and (b) show the current waveforms of the cells \( b \) and \( c \), respectively, for balancing and unbalancing condition. As it can be seen, the output current of the ports are affected by the unbalancing condition only during half switching period. Besides that, the additional charge delivered or removed from each port is highlighted in

![Fig. 5. Current efforts in function of the power: (a) rms current on the primary and secondary side of the QAB converter, (b) rms and mean current on the switches of the MV side of the QAB converter.](image-url)
As it can be observed in (12) and (13), the equations of MV bridges can be used to control the additional power transferred to the case, we have
\[ \Delta P_2 = V_H \frac{\Delta Q_2}{T_s} \rightarrow \Delta Q_2 = \int_{T_c/2}^{T_c} ib(t)dt \]  \hspace{1cm} (19)
\[ P_2 = \frac{P_1}{3} + \Delta P_2 \]  \hspace{1cm} (20)

The power processed by the cell b is composed by the total balanced power (given by \( P_1/3 \)) and an additional power portion \( \Delta P_2 \), as presented in (20). The variable \( \Delta P_2 \) is responsible for the unbalancing power and for power balanced case, we have \( \Delta P_2 = 0 \). The additional power \( \Delta P_2 \) is calculated using the additional charge shown in Fig. 7 (b) as presented in (19). The additional charge is also shown in equation (19). Therefore, solving (19), it is found the equation of \( \Delta P_2 \) in function of \( \Delta D_2 \), as shown in (21). The same procedure can be done to the power transferred by the cell c and as a result, the power processed by the cell c is given by (21). As it can be observed in (12) and (13), the equations of the additional power are in function of \( \Delta D_2 \), then this variable can be used to control the additional power transferred to the MV bridges.
\[ \Delta P_2 = \frac{3V_H \Delta D_2 (D_2 - \Delta D_2)}{2Lf_s} \]  \hspace{1cm} (21)
\[ \Delta P_3 = \frac{3V_H \Delta D_2 (\Delta D_2 - D_2)}{4Lf_s} \]  \hspace{1cm} (22)

IV. SIMULATION AND EXPERIMENTAL RESULTS

To evaluate the performance of the Quad-Active-Bridge converter using the described modulation strategy and also to verify the theoretical analysis developed in this paper, simulation and experimental results were obtained and they will be discussed in this section.

A. Simulation Results

The simulations was carried out with MATLAB/Simulink and the PLECS toolbox and it is based on the parameters specified in Table II. In addition, leakage inductance of 10 \( \mu \)H and transformer ratio of \( n = 2.63 \) were used.

Fig. 8 (a) to (c) shows the main waveforms in steady-state of the QAB under balancing condition, while Fig. 8 (d) to (e) shows the same waveforms for unbalancing condition. In Fig. 8 (a), it is depicted the voltages \( v_a, v_b \) and \( v_x \) ans the currents \( i_a, i_b, i_c, i_d \) and their switching operation is clearly observed and waveforms are similar to those theoretical ones shown in Fig. 6. The current and voltage waveforms on the switches of the MV bridge and LV bridge are presented in the Fig. 8 (b) and (c), respectively. In this figures, the soft-switching feature is lost. The hard-switching commutation effect can be clearly observed on the waveforms of the voltage \( v_x \) (Fig. 8 (d) on top), in which more levels are presented on this waveforms, and also on the waveforms of the currents \( i_b \) and \( i_c \). The waveforms obtained by simulation are identical to the theoretical one shown in Fig. 6. The current and voltage waveforms on the switches of the MV bridge and LV bridge are presented in the Fig. 8 (e) and (f). In this condition, the soft-switching feature is lost. The hard-switching commutation is even more clear to be observed in the Fig. 8 (f), where the current starts and finish in a value different of zero. Even with a considerably difference of power processed by the cell b and c, the current level on the switches during the commutation is considerably low, implying also in low switching losses.

B. Experimental Results

To evaluate the performance of the Quad-Active-Bridge dc-dc converter experimentally, a downscale prototype was
TABLE III
EXPERIMENTAL SETUP PARAMETERS

<table>
<thead>
<tr>
<th>Specification</th>
<th>Smart Transformer</th>
</tr>
</thead>
<tbody>
<tr>
<td>Power</td>
<td>20 kW</td>
</tr>
<tr>
<td>Input Voltage (MV)</td>
<td>800 V</td>
</tr>
<tr>
<td>Output Voltage (LV)</td>
<td>800 V</td>
</tr>
<tr>
<td>Switching frequency</td>
<td>20 kHz</td>
</tr>
<tr>
<td>Inductance</td>
<td>50 µH</td>
</tr>
<tr>
<td>Transformer turn ratio</td>
<td>n=1</td>
</tr>
</tbody>
</table>

designed, built and experimental results were obtained. The prototype is based on the structure shown in 3 (b), i.e. with HB in the MV side, and it was tested with the triangular current mode modulation strategy for validation purposes. The electrical parameters of the prototype are shown in Table III. The tests were carried out with resistive load. The results were obtained for a input voltage of 250V and output voltage of 200V. The results are depicted in Fig. 9 and 10, for balance and unbalance conditions, respectively.

In Fig. 9, the voltage on LV side (on the cell a) and MV side (on the cells b and c) as well as the current on the LV side i_a are depicted. As can be seen, the voltages v_b and v_c have the same value, indicating balanced condition. In this figure, a perfect triangular current shape is observed and it is very similar to the simulated and theoretical waveforms. Besides that, the soft-switching is clear in this figure.

Finally, the experimental waveform for unbalanced condition operation is shown in Fig. 10, where different value for the voltage v_b and v_c. Besides that, in this condition it is very clear that the converter does not operate at soft-switching anymore, as already discussed.

V. CONCLUSION

In this paper the modulation strategy and operation principle of the medium voltage Quad-Active-Bridge as a solution for the dc-dc conversion stage of smart transformers was presented. The topology presents several advantages in this application, such as soft-switching operation and high power density. In addition, the topology offers an additional power path in the medium voltage side, enabling the power exchange among the MV cells in a efficient way, and increases the redundancy, consequently, the reliability of the system.

The focus of this paper is to study the modulation and operation of the MV QAB dc-dc converter. The triangular current modulation strategy, previously study for the DAB, has its application extended to the QAB converter in this work, where the basic equations of the modulation for this converter are derived.
Moreover, the converter operation at unbalance power is also investigate and a control scheme for balance the voltage in the MV cell is presented. Simulation and experimental results are provided in this paper to attest the theoretical analysis developed herein. The results are in accordance with the theoretical waveforms. As a overall overview, the Quad-Active-Bridge converter has presented high performance with NPC in the MV side, which make it suitable for SST application.

REFERENCES